INSAT

MULTIDESCRIPTIVE CODING TECHNIQUE
FOR MULTISTREAM COMMUNICATION OF SIGNALS

Field of the Invention

The invention relates to communications systems
and methods, and more particularly to systems and methods
for communicating signals through multiple communication
channels.

Background of the Invention

Communication of audio signals plays an important
role in radio and TV broadcast. With the advent of digital
technology, terrestrial and satellite digital audio
broadcast (DAB) systems have been proposed. In prior art,
to efficiently utilize transmission bandwidth to communicate
audio signals, a perceptual audio coding (PAC) technique is
often employed. For details on the PAC technique, one may
refer to U.S. Patent No. 5,285,498 issued February 8, 1994
to Johnston; and U.S. Patent No. 5,040,217 issued August 13,
1991 to Brandenburg et al., both of which are hereby
incorporated by reference. In accordance with such a PAC
technique, each of a succession of time domain blocks of an
audio signal representing audio information is coded in the
frequency domain. Specifically, the frequency domain
representation of each block is divided into coder bands,
each of which is individually coded, based on psycho-
acoustic criteria, in such a way that the audio information
is significantly compressed, thereby requiring a smaller
number of bits to represent the audio information than would
be the case if the audio information were represented in a
more simplistic digital format, such as the PCM format.

In many broadcast systems including the
aforementioned DAB systems, it is possible to transmit audio
signals over multiple alternative channels, which are

simultaneously available for signal transmission. In prior
art, in anticipation of a loss or significant degradation of
a transmitted signal because of imperfect channel
conditions, multiple alternative channels are typically used

5   to transmit duplicate signals, respectively, to realize path
diversity, thereby improving the accuracy of recovery of the
transmitted signal. An example for a realization of path
diversity may be broadcasting duplicate digital audio
signals via multiple satellites in a satellite DAB system.

10   **Summary of the Invention**

We have recognized that the above-described use of
multiple alternative channels in prior art represents an
inefficient utilization of transmission bandwidth especially
when the communication channels are relatively reliable, as

15   are those in a DAB system, e.g., the satellite DAB system.

In accordance with the invention, to utilize
transmission bandwidth efficiently, multidescriptive
representations of a signal for transmission are generated,
and the representations are transmitted through the

20   respective alternative channels, thereby realizing a
"multistream" transmission. In general, the more
representations are received and used to recover the signal,
the higher the quality of the recovered signal.

For example, in a DAB system, in communicating a

25   stereo audio signal which includes a left channel signal and
a right channel signal, at least a first multidescriptive
representation and a second multidescriptive representation
of the signal are generated in accordance with the
invention, and then transmitted through the respective

30   alternative channels in the system. The first
representation contains first information concerning at

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least the left channel signal, and second information concerning at least a first coefficient for predicting the right channel signal based on the first information. Similarly, the second representation containing third

5 information concerning at least the right channel signal, and fourth information concerning at least a second coefficient for predicting the left channel signal based on the third information.

One or more of the transmitted multidescriptive

10 representations of the stereo audio signal received from the channels may be selected for recovering the signal. For example, when the first (second) representation is selected for the signal recovery, the recovered signal includes a recovered left (right) channel signal based on the first

15 (third) information, and a prediction of the transmitted right (left) channel signal based on the first (second) coefficient in the representation, thereby affording an acceptable stereo audio quality. When both the first and second representations are selected for the signal recovery,

20 the recovered signal includes recovered left and right channel signals based on the first and third information in the respective representations, thereby affording a higher stereo audio quality.

Brief Description of the Drawing

25 In the drawing,

Fig. 1 illustrates a satellite digital audio broadcast arrangement in accordance with the invention;

Fig. 2 is a block diagram of a transmitter for transmitting a stereo audio signal in the arrangement of

30 Fig. 1; and

Fig. 3 is a block diagram of a receiver for

recovering the transmitted stereo audio signal in the
arrangement of Fig. 1.

Detailed Description

Fig. 1 illustrates digital broadcast arrangement
5   100 embodying the principles of the invention, e.g., a
satellite digital audio broadcast (DAB) arrangement in this
instance. In arrangement 100, control station 103 generates
DAB signals containing, e.g., stereo audio information, and
transmits the signals through multiple alternative channels
10 which are simultaneously available for signal transmission.
For example, mobile 105, including therein a receiver
described below, may receive the transmitted DAB signals
from control station 103 via satellite links 112 and 115
through satellites 107a and 107b, respectively, and/or radio
15 frequency (RF) link 117 through terrestrial antenna 109.
However, in this particular illustrative embodiment, the
terrestrial transmission serves as a "gap filler" or, in
other words, substitute for the satellite transmissions in
areas where the satellite transmissions cannot reach. To
20 that end, DAB signals containing the stereo audio
information are transported from control station 103 through
cable 120, e.g., a T1 line, to terrestrial antenna 109
located in one such area.

In prior art, multiple alternative channels are
25 typically used to transmit duplicate copies of a signal,
respectively, to realize path diversity in anticipation of a
loss or significant degradation of the transmitted signal
due to imperfect channel conditions, thereby improving the
accuracy of recovery of the transmitted signal. However, we
30 have recognized that such prior art use of the multiple
alternative channels represents an inefficient utilization

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of transmission bandwidth especially when the communication channels are relatively reliable, as are satellite links 112 and 115 in arrangement 100.

     In accordance with the invention, to utilize

5 transmission bandwidth efficiently, multidescriptive representations of a signal for transmission are generated, and the representations are transmitted through the respective alternative channels. In general, the more representations are received and used to recover the signal,

10 the higher the quality (e.g., based on a signal-to-noise ratio or perceptually based measure) of the recovered signal.

     Specifically, in this illustrative embodiment, two multidescriptive representations, referred to as "D1 and D2

15 representations", are used to represent stereo audio information, and the D1 and D2 representations are transmitted through satellite links 112 and 115, respectively. Because of the design of the multidescriptive coding described below, the audio signal recovered based on

20 the D1 representation or D2 representation alone affords an acceptable stereo audio quality. The audio signal recovered based on both the D1 and D2 representations affords a relatively high stereo audio quality.

     Fig. 2 illustrates transmitter 201 in control

25 station 103 for generating and transmitting the D1 and D2 representations in accordance with the invention through satellite links 112 and 115, respectively, and the aforementioned gap filler signal through RF link 117. The D1 and D2 representations contains information concerning an

30 analog stereo audio signal for transmission, which in a conventional manner consists of left channel signal L and right channel signal R, which are fed to transmitter 201.

In accordance with the inventive multidescriptive coding
technique, for example, the D1 representation contains (i)
information concerning L, and (ii) parametric information
concerning R (denoted "param-R") resulting from parametric
5   stereo coding of R with respect to L. Because of the design
of the stereo parametric coding described below, R can be
predicted based on the param-R and L information. As a
result, the stereo audio signal recovered based on the D1
representation alone includes L and a prediction of R,
10   affording an acceptable stereo audio quality, where L is
derived from the L information in the D1 representation, and
the prediction of R is derived from both the param-R and L
information therein.

        Similarly, the D2 representation contains (i)
15   information concerning R, and (ii) parametric information
concerning L (denoted param-L) resulting from parametric
stereo coding of L with respect to R. Because of the design
of the parametric stereo coding, L can be predicted based on
the param-L and R information. As a result, the stereo
20   audio signal recovered based on the D2 representation alone
includes R and a prediction of L, affording an acceptable
stereo audio quality, where R is derived from the R
information in the D2 representation, and the prediction of
L is derived from both the param-L and R information
25   therein.

        In addition, the stereo audio signal recovered
based on both the D1 and D2 representations includes L
derived from the L information in the D1 representation, and
R derived from the R information in the D2 representation,
30   affording a relatively high stereo audio quality. The
redundant param-R and param-L information in the respective
D1 and D2 representations may further be utilized for

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additional high frequency stereo image correction to afford an even higher stereo audio quality.

The above parametric stereo coding is predicated upon an observation that in frequency domain the content of L can be predicted from that of R, and vice versa. Thus, without loss of generality, param-R in the D1 representation may be derived based on the following relation:

$$R_f = \alpha L_f \ , \qquad (1)$$

where R_f represents the frequency spectrum of R, L_f represents the frequency spectrum of L, and α represents a predictor coefficient from which param-R is derived. To improve the prediction of R_f based on L_f in (1), multiple predictor coefficients across the frequency range may be used, and hence:

$$R_f^i = \alpha^i L_f^i \ , \qquad (2)$$

where i represents an index for an ith prediction frequency band in the frequency range. For example, where a perceptual audio coding (PAC) technique is applied to an audio signal, which is the case here and described below, each ith prediction frequency band may coincide with a different one of the coder bands which approximate the well known critical bands of the human auditory system, in accordance with the PAC technique.

Referring to expression (2), the success of predicting R_f^i depends on how well the predictor coefficients, α^i, can capture the stereo cues in the signal. As is well known, stereo localization is based on both magnitude and phase cues. An enhanced prediction scheme for well capturing both magnitude and phase cues will now be described. This scheme relies on imposing some constraints

on L and R so that both magnitude information and phase information thereof are available in a single domain to perform the prediction. It is well known in the signal processing theory that if a real signal satisfies a

5 "causality constraint," the real part of the signal spectrum provides a sufficient representation thereof as the imaginary part of the spectrum may be recovered based on the real part without any additional information. Thus, the enhanced prediction scheme in question may be mathematically

10 expressed as follows:

$$R^i_{f\ real-causal} = \alpha^i L^i_{f\ real-causal} \quad . \quad (3)$$

Based on expression (3), the aforementioned parametric stereo coding is achieved by computing the predictor coefficients α^i from the real parts of L^i_f and R^i_f after the causality constraints are respectively imposed onto L and R

15 in the time domain, and param-R comprises information concerning α^i for each ith prediction frequency band.

It should be pointed out at this juncture that in practice, the imposition of a causality constraint on L (or R) in the time domain is readily accomplished by zero

20 padding the samples representing L (or R). Thus, in a well known manner, $L^i_{f\ real-causal}$ (or $R^i_{f\ real-causal}$) is realized by appending "zeros" to a block of N samples representing L to lengthen the block to (2N-1) samples long, followed by a frequency transform of the zero-padded block and extraction

25 of the real part of the resulting transform, where N is a predetermined number.

For an even more enhanced prediction, a multi-tap predictor may be utilized whereby α^i represents a set of predictor coefficients for an ith prediction frequency band.

30 For example, where a 2-tap predictor is used, $\alpha^i = [\alpha^i_0 \ \alpha^i_1]$

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which may be expressed as follows:

$$r = \alpha_0^i \ell + \alpha_1^i \ell' \ , \qquad (4)$$

where r represents the set of real parts of the frequency components in $R^i_{f\ real\text{-}causal}$ in the ith prediction band, ℓ represents the set of real parts of the frequency components

5   in $L^i_{f\ real\text{-}causal}$ in the ith prediction band, ℓ' represents the set of real parts of the frequency components in $L^i_{f\ real\text{-}causal}$ in the $(i-1)^{th}$ prediction band. As such, the predictor coefficients α^i_0 and α^i_1 may be determined by solving the following equation:

$$\begin{bmatrix} \ell^T\ell & \ell^T\ell' \\ \ell^T\ell' & \ell'^T\ell' \end{bmatrix} \begin{bmatrix} \alpha_0^i \\ \alpha_1^i \end{bmatrix} = \begin{bmatrix} \ell^T r \\ \ell'^T r \end{bmatrix} \ , \qquad (5)$$

10   where the superscript "T" denotes a standard matrix transposition operation. Thus,

$$\begin{bmatrix} \alpha_0^i \\ \alpha_1^i \end{bmatrix} = G^{-1}H \ , \qquad (6)$$

where

$$G = \begin{bmatrix} \ell^T\ell & \ell^T\ell' \\ \ell^T\ell' & \ell'^T\ell' \end{bmatrix} \ ;$$

$$H = \begin{bmatrix} \ell^T r \\ \ell'^T r \end{bmatrix} \ ;$$

and the superscript "-1" denotes a standard matrix inverse operation.

15   In this illustrative embodiment, param-R in the D1 representation comprises information concerning predictor coefficients α^i_0 and α^i_1 for predicting R based on the L information in the D1 representation. Based on the

disclosure heretofore, it is apparent to a person skilled in the art that param-L in the D2 representation comprises information concerning predictor coefficients β^i_0 and β^i_1 for predicting L based on the R information in the D2

5   representation, where β^i_0 and β^i_1 are obtained similarly to α^i_0 and α^i_1 using equation [6] with "ℓ" and "r" interchanged.

For example, if each alternative communication channel affords a bit rate of 64 kbps, for the D1 representation, 56-60 kbps may be allocated to the

10   transmission of the L information and 4-8 kbps to the transmission of param-R. Similarly, for the D2 representation, 56-60 kbps may be allocated to the transmission of the R information, and 4-8 kbps to the transmission of param-L.

15   Referring back to equation (6), it can be shown that if L is weak, and thus det G (i.e, determinant of G) has a small value, equation (6) for solving α^i_0 and α^i_1 would be numerically ill conditioned. As a consequence, use of the resulting α^i_0 and α^i_1, and thus param-R, to predict R

20   based on L is not viable.

To avoid the numerically ill condition in (6), a second multidescriptive coding technique in accordance with the invention will now be described. According to this second technique, the D1 representation contains (i)

25   information concerning L*, and (ii) parametric information concerning R resulting from parametric stereo coding of R with respect to L*, denoted param-R[w.r.t. L*], where, e.g.,

$$L^* = aL + bR , \qquad (7)$$

where a + b = 1 and a >> b $\geq$ 0. In addition, the D2 representation contains (i) information concerning R*, and

30   (ii) parametric information concerning L resulting from

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parametric stereo coding of L with respect to R*, denoted param-L[w.r.t. R*], where, e.g.,

$$R^* = aR - bL \ . \qquad (8)$$

5 It should be noted that the multidescriptive coding technique previously described is merely a special case of the second technique with a = 1 and b = 0. In any event, the disclosure hereupon is based on the generalized, second multidescriptive coding technique involving R* and L*.

10 It should also be noted that it may be more advantageous to employ the generalized multidescriptive coding technique especially when a stereo signal includes an extremely strong stereo tilt (i.e., almost completely dominated by either L or R). By controlling the a and b values, the pair L* and R* in accordance with the
15 generalized technique exhibits a reduced stereo separation, thereby increasing the "naturalness" of the parametric stereo coding. If both the D1 and D2 representations are used for signal recovery, the R and L pair can be reconstructed based on the R* and L* information in the D1
20 and D2 representations, respectively. When the D1 (or D2) representation alone is used for signal recovery, the prediction of R (or L) based on param-R[w.r.t. L*] (or param-L[w.r.t. R*]) in the D1 (or D2) representation leads to a more natural audio effect. As fully described below,
25 the a and b values are adaptively selected depending on the specific L and R values. Similarly, if each alternative communication channel affords a bit rate of 64 kbps, for the D1 (or D2) representation, 56-60 kbps may be allocated to the transmission of the L* (or R*) information, and 4-8 kbps
30 to the transmission of param-R[w.r.t. L*] (or param-L[w.r.t.

R*]).

Referring back to Fig. 2., the aforementioned L
and R are fed to multidescriptive coder 203 in transmitter
201. In response, analog-to-digital (A/D) convertor 205 in
5   coder 203 digitizes L and R, thereby providing PCM samples
of L and R denoted L(n) and R(n), respectively, where n
represents an index for an nth sample interval. Based on
L(n) and R(n), mixer 207 generates L*(n) on lead 209a in
accordance with expression (7) above, and R*(n) on lead 209d
10   in accordance with expression (8) above, where values of a
and b are adaptively selected by adapter 211 described
below. In addition, R(n) and L(n) bypass mixer 207 onto
leads 209b and 209c, respectively. Leads 209a-209d extend,
and thereby provide the respective L*(n), R(n), L(n) and
15   R*(n), to parametric stereo coder 215 described below.
L*(n) and R*(n) are also provided to PAC coder 217 and 219,
respectively.

In a conventional manner, PAC coder 217 divides
the PCM samples L*(n) into time domain blocks, and performs
20   a modified discrete cosine transform (MDCT) on each block to
provide a frequency domain representation therefor. The
resulting MDCT coefficients are grouped according to coder
bands for quantization. As mentioned before, these coder
bands approximate the well known critical bands of the human
25   auditory system. PAC coder 217 also analyzes the audio
signal samples, L*(n), to determine the appropriate level of
quantization (i.e., quantization stepsize) for each coder
band. This level of quantization is determined based on an
assessment of how well the audio signal in a given coder
30   band masks noise. The quantized MDCT coefficients then
undergo a conventional Huffman compression process,
resulting in a bit stream representing L* on lead 222a.

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Similarly, PAC coder 219 processes the PCM samples $R*(n)$, resulting in another bit stream representing $R*$ on lead 222d.

Based on received $L*(n)$ and $R(n)$, parametric
5   stereo coder 215 generates parametric signals $P*_R$. Similarly, based on received $R*(n)$ and $L(n)$, coder 215 generates $P*_L$. Signal $P*_R$ contains information concerning param-R[w.r.t. $L*$] which comprises predictor coefficients α^i_0 and α^i_1 in accordance with equation (6) above, although
10   "ℓ" and "ℓ'" therein are derived from $L*$ here, rather than L, pursuant to the generalized multidescriptive coding technique. Similarly, signal $P*_L$ contains information concerning param-L[w.r.t. $R*$] which comprises predictor coefficients β^i_0 and β^i_1 (replacing α^i_0 and α^i_1) in accordance
15   with equation (6) with "ℓ" and "r" therein interchanged and with the resulting "r" and "r'" derived from $R*$, rather than R, pursuant to the generalized multidescriptive coding technique.

Signals $P*_R$ and $P*_L$ are quantized by conventional
20   nonlinear quantizers 225 and 227, respectively, thereby providing a bit stream representing $P*_R$ on lead 222b, and another bit stream representing $P*_L$ on lead 222c. Leads 222a and 222b extend to D1 formatter 231 where for each time domain block, the bit stream representing $P*_R$ on lead 222b
25   corresponding to the time domain block is appended to that representing $L*$ on lead 222a corresponding to the same time domain block, resulting in the aforementioned D1 representation. Similarly, leads 222c and 222d extend to D2 formatter 233 where the bit stream representing $P*_L$ on lead
30   222c is appended to that representing $R*$ on lead 222d, resulting in the aforementioned D2 representation.

The adaptation algorithm implemented by adapter

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211 for selecting the values of a and b will now be described. This adaptation algorithm involves finding a smooth estimate of an upcoming value of a = a_{cur+1}, which is a function of the current time domain blocks of L*(n) and

5   R*(n) being processed by parametric stereo coder 215, in accordance with the following iterative process:

$$a_{cur+1} = \gamma \varepsilon_{cur} + (1 - \gamma) a_{cur} \quad , \qquad (9)$$

and

$$a_0 = 1 \quad ,$$

where cur represents an iterative index greater than or equal to zero; γ represents a constant having a value close

10   to one, e.g., γ = 0.95 in this instance; and ε_{cur} is defined as follows:

$$\varepsilon_{cur} = 0.5 + 0.5 \left| \frac{\mathcal{L}*(f) \cdot \mathfrak{R}*(f)}{\|\mathcal{L}*(f)\| \, \|\mathfrak{R}*(f)\|} \right| \quad ,$$

where $\mathcal{L}*(f)$ and $\mathfrak{R}*(f)$ respectively are spectrum representations of the current time domain blocks of L*(n) and R*(n) in the form of vectors; " $\cdot$ " represents a standard

15   inner product operation; and $\|\mathcal{L}*(f)\|$ and $\|\mathfrak{R}*(f)\|$ represent the magnitudes of $\mathcal{L}*(f)$ and $\mathfrak{R}*(f)$, respectively.

Since a + b = 1 as mentioned before, the value selected by adapter 211 for b simply equals 1 - a. It should be noted that alternatively, a and b may be

20   predetermined constant values, thereby obviating the need of adapter 211.

The aforementioned gap-filler signal is realized by encoding L and R using conventional stereo source coder 241. The resulting bit stream from coder 241 is hereinafter

25   referred to as a "D3 representation."

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The D1, D2 and D3 representations are fed to outer
channel coder 251a, outer channel coder 251b and outer
channel coder 251c, respectively. Outer channel coder 251a
encodes the D1 representation according to a well known
5   forward error correction coding technique, e.g., the Reed
Solomon coding technique in this instance, or alternatively
a binary cyclic redundancy check (CRC) block coding
technique, to afford correction and/or detection of errors
in the D1 representation after its transmission. The D1
10   representation is processed by coder 251a on a block by
block basis, with each block having a predetermined number
of bits. In a conventional manner, coder 251a appends the
Reed Solomon check symbols resulting from the encoding of
each corresponding block. Similarly, coders 251b and 251c
15   respectively processes the D2 and D3 representations on a
block by block basis, and append Reed Solomon check symbols
to each corresponding block of the representations for error
correction and/or detection purposes.

The Reed Solomon coded D1 representation, Reed
20   Solomon coded D2 representation and Reed Solomon coded D3
representation are fed to inner convolutional coders 253a,
253b and 253c, respectively. Inner convolutional coder 253a
processes the received Reed Solomon coded D1 representation
on a symbol (different from a Reed Solomon check symbol)
25   interval by symbol interval basis, where the symbol interval
has a predetermined duration T_1.

Coder 253a encodes the received bit stream in
accordance with a well known convolutional code to provide
the communications system with a so-called "coding gain"
30   which manifests itself in the form of enhance immunity to
such random channel impairments as additive noise, without
sacrificing the source bit rate or additional broadcast

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bandwidth. Specifically, coder 253a introduces redundancy into the received bit stream in accordance with the convolutional code to allow use of a maximum likelihood decoding technique at receiver 303 in Fig. 3 to be

5   described. During each symbol interval, coder 253a forms an encoded word, which includes bits from the received Reed Solomon coded D1 representation and is used to select a symbol from a signal constellation in accordance with a well known digital modulation scheme, e.g., a quaternary phase

10   shift keying (QPSK) scheme. Specifically, the symbols in a QPSK signal constellation each have the same signal level but their phases are spaced $\pi/2$ radians apart. The selected symbols from coder 253a are interleaved by interleaver 255a to pseudo-randomize the symbols. QPSK modem 257a processes

15   the symbols from interleaver 255a and generates digitally modulated signals corresponding to such symbols. The digitally modulated signals are transmitted by transmit circuit 259a via satellite link 112. Transmit circuit 259a includes, e.g., a satellite up-converter, a power amplifier,

20   a satellite antenna, etc., all of conventional design.

Similarly, during each symbol interval T_2 (in this instance, $T_1 = T_2$), inner convolutional coder 253b forms an encoded word, which includes bits from the received Reed Solomon coded D2 representation and is used to select a

25   symbol from a second QPSK signal constellation. The resulting sequence of selected symbols are interleaved by interleaver 255b to pseudo-randomize the symbols. QPSK modem 257b processes the symbols from interleaver 255b and generates digitally modulated signals corresponding to such

30   symbols. The digitally modulated signals are transmitted via satellite link 115 by transmit circuit 259b, which includes, e.g., a satellite up-converter, a power amplifier,

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a satellite antenna, etc., all of conventional design.

In addition, during each symbol interval T_3, inner convolutional coder 253c similarly forms an encoded word, which includes the received Reed Solomon coded D3

5   representation and is used to select a symbol from a third predetermined signal constellation, which may not be a QPSK signal constellation in this instance. The resulting sequence of selected symbols are interleaved by interleaver 255c to pseudo-randomize the symbols. During each time

10   frame which is KT_3 long, OFDM modem 257c transmits K symbols from interleaver 255c in accordance with the well known orthogonal frequency division multiplexed (OFDM) scheme, where K is a predetermined number. In a well known manner, modem 257c generates K pulse shaping carriers corresponding

15   to the K_3 symbols. The resulting pulse shaping carriers are transmitted via RF link 117 by transmit circuit 259c, which includes, e.g., an RF up-converter, a power amplifier, terrestrial antenna 109, etc., all of conventional design.

Referring to Fig. 3, receiver 303 which resides in

20   mobile 105 receives signals transmitted by transmitter 201 through satellite links 112 and 115, and/or RF link 117. The received signals corresponding to the D1 representation, D2 representation and D3 representation are processed by receive circuits 307a, 307b and 307c, which perform inverse

25   functions to above-described transmit circuits 259a, 259b and 259c, respectively. The output of circuit 307a comprises the digitally modulated signals as transmitted by transmit circuit 259a, which are fed to demodulator 309a. Accordingly, demodulator 309a generates a sequence of

30   symbols corresponding to the D1 representation. The generated symbols are de-interleaved by de-interleaver 313a which performs the inverse function to interleaver 255a

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described above. Based on the de-interleaved symbols and
the corresponding signal constellation used, inner
convolutional decoder 217a in a conventional manner
determines what the most likely transmitted symbols are,

5   thereby recovering the D1 representation incorporating Reed
Solomon check symbols therein, i.e., the Reed Solomon coded
D1 representation. Outer channel decoder 219a extracts the
Reed Solomon check symbols from blocks of the Reed Solomon
coded D1 representation, and examines the Reed Solomon check

10   symbols in connection with the corresponding blocks of the
D1 representation. Each block of the D1 representation may
be corrupted and contain errors because of channel
imperfections, e.g., interference in satellite link 112. If
the number of errors in each block is smaller than a

15   threshold whose value depends on the actual Reed Solomon
coding technique used, decoder 319a corrects the errors in
the block. However, if the number of errors in each block
is larger than the threshold and the errors are detected by
decoder 319a, the latter issues, to blending processor 327

20   described below, a first flag indicating the error
detection. Decoder 319a then provides the recovered D1
representation to multidescriptive decoder 230.

Similarly, the output of circuit 307b comprises
the digitally modulated signals corresponding to the D2

25   representation, which are fed to demodulator 309b.
Accordingly, demodulator 309b generates a sequence of
symbols corresponding to the D2 representation. The
generated symbols are de-interleaved by de-interleaver 313b
which performs the inverse function to interleaver 255b

30   described above. Based on the de-interleaved symbols and
the corresponding signal constellation used, inner
convolutional decoder 317b in a conventional manner

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determines what the most likely transmitted symbols are, thereby recovering the D2 representation incorporating Reed Solomon check symbols therein, i.e., the Reed Solomon coded D2 representation. Outer channel decoder 219b extracts the

5   Reed Solomon check symbols from blocks of the Reed Solomon coded D2 representation, and examines the Reed Solomon check symbols in connection with the corresponding blocks of the D2 representation. Each block of the D2 representation may be corrupted and contain errors because of channel

10   imperfections. If the number of errors in each block is smaller than the aforementioned threshold, decoder 319b corrects the errors in the block. However, if the number of errors in each block is larger than the threshold and the errors are detected by decoder 319b, the latter issues, to

15   blending processor 327, a second flag indicating the error detection. Decoder 319b then provides the recovered D2 representation to multidescriptive decoder 330.

In addition, the output of circuit 307c comprises the K pulse shaping carriers corresponding to the D3

20   representation, which are fed to demodulator 309c. Accordingly, demodulator 309c generates a sequence of K symbols corresponding to the D3 representation. The generated symbols are de-interleaved by de-interleaver 313c which performs the inverse function to interleaver 255c

25   described above. Based on the de-interleaved symbols and the corresponding signal constellation used, inner convolutional decoder 317c in a conventional manner determines what the most likely transmitted symbols are, thereby recovering the D3 representation incorporating Reed

30   Solomon check symbols therein, i.e., the Reed Solomon coded D3 representation. Outer channel decoder 319c extracts the Reed Solomon check symbols from blocks of the Reed Solomon

coded D3 representation, and examines the Reed Solomon check
symbols in connection with the corresponding blocks of the
D3 representation. Each block of the D3 representation may
be corrupted and contain errors because of channel

5   imperfections. If the number of errors in each block is
smaller than the aforementioned threshold, decoder 319c
corrects the errors in the block. However, if the number of
errors in each block is larger than the threshold and the
errors are detected by decoder 319c, the latter issues, to

10   blending processor 327, a third flag indicating the error
detection. Decoder 319c then provides the recovered D3
representation to conventional stereo source decoder 335.
By performing the inverse function to stereo source coder
241 described above, decoder 335 recovers the stereo audio

15   signal which has components corresponding to L and R and
which serves as a gap filler as mentioned before. The gap-
filler stereo audio signal is further processed by
multidescriptive decoder 330.

Multidescriptive decoder 330, among others,

20   performs the inverse function to multidescriptive coder 203
described above and is capable of blending the received D1
representation and D2 representation to recover the
transmitted stereo audio signal. However, blending
processor 327 determines whether the D1 representation is to

25   be blended with the D2-representation in decoder 330, and
whether the gap-filler stereo audio signal, if any, from
stereo source decoder 335 is used for the output. Such a
determination is based on measures of data integrity of the
D1 representation, D2 representation and D3 representation.

30   To that end, processor 527 provides first, second and third
control signals indicative of the determinations of use of
the D1 representation and/or D2 representation in decoder

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330 to recover the stereo audio signal, or the gap filler
stereo audio signal corresponding to the D3 representation
for the output. In response to such control signals,
decoder 330 accordingly (a) utilizes either the D1

5   representation or D2 representation to recover the stereo
audio signal to afford an acceptable stereo audio quality,
(b) utilizes both the D1 representation and D2
representation to recover the stereo audio signal to afford
a higher stereo audio quality, (c) recovers no stereo audio

10   signal based on D1 representation and/or D2 representation,
and utilizes the gap-filler stereo audio signal for the
output, or (d) recovers no stereo audio signal, utilizes no
gap-filler stereo audio signal for the output especially
where no such gap-filler signal is provided, and, instead,

15   performs well known audio concealment for the current symbol
intervals, e.g., interpolation based on the results of audio
recovery in neighboring symbol intervals.

          The measures based on which processor 327
determines whether any of the D1 representation and D2

20   representation is used in recovering the stereo audio
signal, and whether any gap-filler stereo audio signal
corresponding to the D3 representation is used for the
output include, e.g., the frequencies of the first, second
and third flags received by processor 327, which are

25   indicative of bit errors in the received D1 representation,
D2 representation and D3 representation, respectively. The
actual frequency threshold beyond which the corresponding
representation is rejected depends on the bit rate of the
representation, output quality requirements, etc.

30   The aforementioned measures may also include an
estimate of a signal-to-interference ratio concerning each
channel obtained during periodic training of each of modems

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257a, 257b and 257c. Since these modems may implement
multilevel signaling and operate in varying channel
conditions, a training sequence with known symbols is used
for equalization and level adjustments in demodulators 309a,
5   309b and 309c periodically. Such a training sequence can be
used to estimate the signal-to-interference ratio. With
QPSK signaling, an automatic gain control (AGC) or some
receiver signal measurement may alternatively be used. When
such an estimate goes below an acceptable threshold,
10   blending processor 327 receives an exceptional signal from
the corresponding demodulator. In response to the
exceptional signal, and depending on other measures,
processor 327 may issue a control signal concerning the
representation associated with the demodulator to cause
15   decoder 330 to reject the representation. As the
exceptional signal needs to be time aligned with the portion
of the representation affected by the substandard signal-to-
interference ratio, delay element 335 is employed to
compensate for the delay imparted to such a representation
20   portion in traversing the deinterleaver and intervening
decoders.

        The foregoing merely illustrates the principles of
the invention. It will thus be appreciated that those
skilled in the art will be able to devise numerous other
25   schemes which embody the principles of the invention and are
thus within its spirit and scope.

        For example, it will be appreciated that in
recovering the stereo audio signal, the D3 representation
may be blended with either D1 or D2 representation. In that
30   case, the D3 representation may add stereo information to,
and/or reduce the quantization noise in, the D1
representation (or D2 representation) for an increased

stereo audio quality.

It will also be appreciated that there may be no gap filler signal and thus no D3 representation in certain locations.

5   In addition, in the illustrative embodiment, D1 and D2 representations are transmitted in accordance with a QPSK scheme. It will be appreciated that one skilled in the art may utilize instead other schemes such as a trellis coded modulation (TCM) scheme with higher order modulation

10   such as 8-PSK, etc.

Moreover, the invention is illustrated in the context of a satellite broadcast system. However, the inventive multidescriptive coding technique described above may also be applied to other communications and broadcast

15   systems, e.g., terrestrial FM and AM, and Internet broadcast systems. For example, the representations resulting from the inventive multidescriptive coding may be respectively transmitted in bands adjacent to and on either side of the power spectrum of a host analog FM signal, in accordance

20   with a prior art in band on channel (IBOC) scheme. In addition, the inventive multidescriptive coding technique may be used in conjunction with the quantizer based multidescriptive technique disclosed in the commonly assigned U.S. Application Serial No. 09/280,280, filed on

25   March 29, 1999.

Further, the multidescriptive representations of a signal, e.g., the D1 and D2 representations, in accordance with the invention may be transmitted through the same communication channel, e.g., the same satellite link, with a

30   time delay for achieving robustness against short time outages.

Finally, transmitter 201 and receiver 303 are

disclosed herein in a form in which various system functions are performed by discrete functional blocks. However, any one or more of these functions could equally well be embodied in an arrangement in which the functions of any one

5   or more of those blocks or indeed, all of the functions thereof, are realized, for example, by one or more appropriately programmed processors.